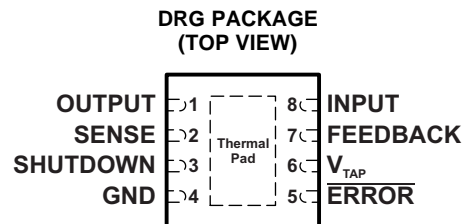


## ADJUSTABLE MICROPOWER VOLTAGE REGULATORS WITH SHUTDOWN

Check for Samples: [LP2951-33-Q1](#), [LP2951-50-Q1](#)

### FEATURES

- Qualified for Automotive Applications
- Wide Input Range: Up to 35 V
- Rated Output Current of 100 mA
- Low Dropout: 380 mV (Typ) at 100 mA
- Low Quiescent Current: 75  $\mu$ A (Typ)
- Tight Line Regulation: 0.03% (Typ)
- Tight Load Regulation: 0.04% (Typ)
- High  $V_O$  Accuracy
  - 1.4% at 25°C
  - 2% Over Temperature
- Can Be Used as a Regulator or Reference
- Stable With Low ESR ( $>12\text{ m}\Omega$ ) Capacitors
- Current- and Thermal-Limiting Features
- 8-Pin Package
  - Fixed Voltages: 5 V/ADJ and 3.3 V/ADJ
  - Low-Voltage Error Signal on Falling Output
  - Shutdown Capability
  - Remote Sense Capability for Optimal Output Regulation and Accuracy



### DESCRIPTION

The LP2951-xx-Q1 devices are bipolar, low-dropout voltage regulators that can accommodate a wide input supply-voltage range of up to 35 V. The 8-pin LP2951-xx-Q1 is able to output either a fixed or adjustable output from the same device. By tying the OUTPUT and SENSE pins together, and the FEEDBACK and  $V_{TAP}$  pins together, the LP2951-xx-Q1 outputs a fixed 5 V and 3.3 V (depending on the version). Alternatively, by leaving the SENSE and  $V_{TAP}$  pins open and connecting FEEDBACK to an external resistor divider, the output can be set to any value between 1.235 V to 30 V.

The 8-pin LP2951-xx-Q1 also offers additional functionality that makes it particularly suitable for battery-powered applications. For example, a logic-compatible shutdown feature allows the regulator to be put in standby mode for power savings. In addition, there is a built-in supervisor reset function in which the ERROR output goes low when  $V_{OUT}$  drops by 6% of its nominal value for whatever reasons – due to a drop in  $V_{IN}$ , current limiting, or thermal shutdown.

The LP295x-xx-Q1 devices are designed to minimize all error contributions to the output voltage. With a tight output tolerance (0.5% at 25°C), a very low output voltage temperature coefficient (20 ppm typical), extremely good line and load regulation (0.3% and 0.4% typical), and remote sensing capability, the parts can be used as either low-power voltage references or 100-mA regulators.

For the most-current package and ordering information, see the Package Option Addendum at the end of this document, or see the TI Web site at [www.ti.com](http://www.ti.com).

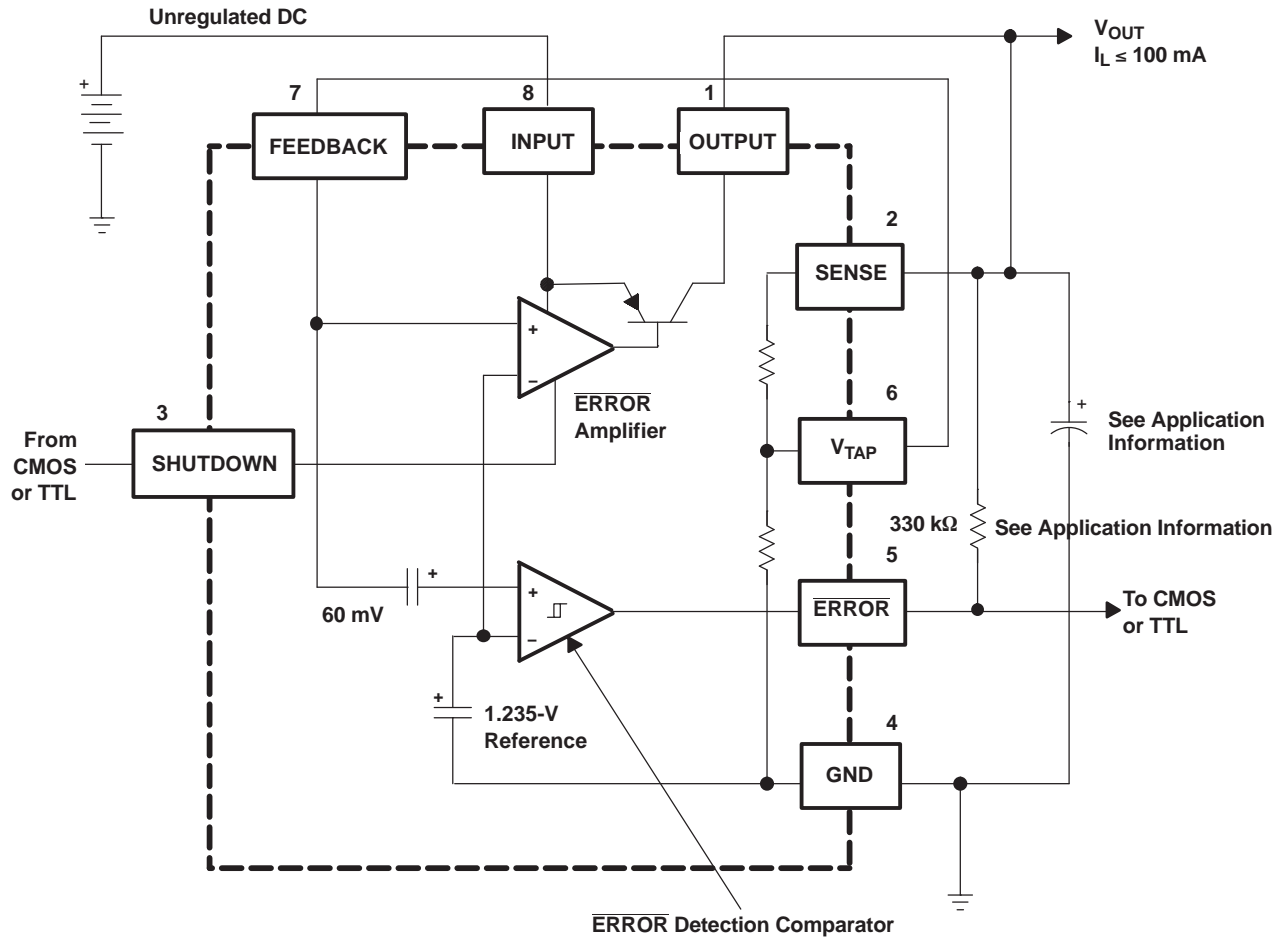


Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

## FUNCTIONAL BLOCK DIAGRAM



## ABSOLUTE MAXIMUM RATINGS<sup>(1)</sup>

over operating free-air temperature range (unless otherwise noted)

$V_{IN}$	Input voltage range	–0.3 V to 35 V
$V_{SHDN}$	SHUTDOWN input voltage range	–1.5 V to 35 V
$\overline{ERROR}$	comparator output voltage range <sup>(2)</sup>	–1.5 V to 30 V
$V_{FDBK}$	FEEDBACK input voltage range <sup>(2) (3)</sup>	–1.5 V to 30 V
$T_J$	Operating virtual-junction temperature	150°C
$T_{stg}$	Storage temperature range	–65°C to 150°C

- (1) Stresses beyond those listed under "absolute maximum ratings" may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under "recommended operating conditions" is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) May exceed input supply voltage
- (3) If load is returned to a negative power supply, the output must be diode clamped to GND.

## RECOMMENDED OPERATING CONDITIONS

		MIN	MAX	UNIT
$V_{IN}$	Supply input voltage	See <sup>(1)</sup>	30	V
$T_A$	Operating temperature	–40	125	°C

- (1) Minimum  $V_{IN}$  is the greater of:  
(a) 2 V (25°C), 2.3 V (over temperature), or  
(b)  $V_{OUT(MAX)} + \text{Dropout (Max)}$  at rated  $I_L$

## THERMAL INFORMATION

THERMAL METRIC		LP2951-xx-Q1	UNIT
		DRG 8 PINS	
$\theta_{JA}$	Junction-to-ambient thermal resistance	55.7	°C/W
$\theta_{JCTop}$	Junction-to-case (top) thermal resistance	66.5	
$\theta_{JB}$	Junction-to-board thermal resistance	30.2	
$\psi_{JT}$	Junction-to-top characterization parameter	1.1	
$\psi_{JB}$	Junction-to-board characterization parameter	30.4	
$\theta_{JCbott}$	Junction-to-case (bottom) thermal resistance	10	

## ELECTRICAL CHARACTERISTICS

$V_{IN} = V_{OUT} \text{ (nominal)} + 1 \text{ V}$ ,  $I_L = 100 \mu\text{A}$ ,  $C_L = 1 \mu\text{F}$  (5-V versions) or  $C_L = 2.2 \mu\text{F}$  (3.3-V versions),  
8-pin version: FEEDBACK tied to  $V_{TAP}$ , OUTPUT tied to SENSE,  $V_{SHUTDOWN} \leq 0.7 \text{ V}$

PARAMETER		TEST CONDITIONS	T <sub>A</sub>	MIN	TYP	MAX	UNIT
3.3-V VERSION (LP2951-33)							
V <sub>OUT</sub>	Output voltage	I <sub>L</sub> = 100 μA	25°C	3.267	3.3	3.333	V
			−40°C to 125°C	3.234	3.3	3.366	
5-V VERSION (LP2951-50)							
V <sub>OUT</sub>	Output voltage	I <sub>L</sub> = 100 μA	25°C	4.950	5	5.050	V
			−40°C to 125°C	4.900	5	5.100	
ALL VOLTAGE OPTIONS							
	Output voltage temperature coefficient <sup>(1)</sup>	I <sub>L</sub> = 100 μA	−40°C to 125°C		20	100	ppm/°C
	Line regulation <sup>(2)</sup>	V <sub>IN</sub> = [V <sub>OUT(NOM)</sub> + 1 V] to 30 V	25°C		0.03	0.2	%V
			−40°C to 125°C			0.4	
	Load regulation <sup>(2)</sup>	I <sub>L</sub> = 100 μA to 100 mA	25°C		0.04	0.2	%
			−40°C to 125°C			0.3	
V <sub>IN</sub> − V <sub>OUT</sub>	Dropout voltage <sup>(3)</sup>	I <sub>L</sub> = 100 μA	25°C		50	80	mV
			−40°C to 125°C			150	
		I <sub>L</sub> = 100 mA	25°C		380	450	
			−40°C to 125°C			600	
I <sub>GND</sub>	GND current	I <sub>L</sub> = 100 μA	25°C		75	120	μA
			−40°C to 125°C			140	
		I <sub>L</sub> = 100 mA	25°C		8	12	mA
			−40°C to 125°C			14	
	Dropout ground current	V <sub>IN</sub> = V <sub>OUT(NOM)</sub> − 0.5 V, I <sub>L</sub> = 100 μA	25°C		110	170	μA
			−40°C to 125°C			200	
	Current limit	V <sub>OUT</sub> = 0 V	25°C		160	200	mA
			−40°C to 125°C			220	

- (1) Output or reference voltage temperature coefficient is defined as the worst-case voltage change divided by the total temperature range.  
(2) Regulation is measured at constant junction temperature, using pulse testing with a low duty cycle. Changes in output voltage due to heating effects are covered under the specification for thermal regulation.  
(3) Dropout voltage is defined as the input-to-output differential at which the output voltage drops 100 mV, below the value measured at 1-V differential. The minimum input supply voltage of 2 V (2.3 V over temperature) must be observed.

## ELECTRICAL CHARACTERISTICS (continued)

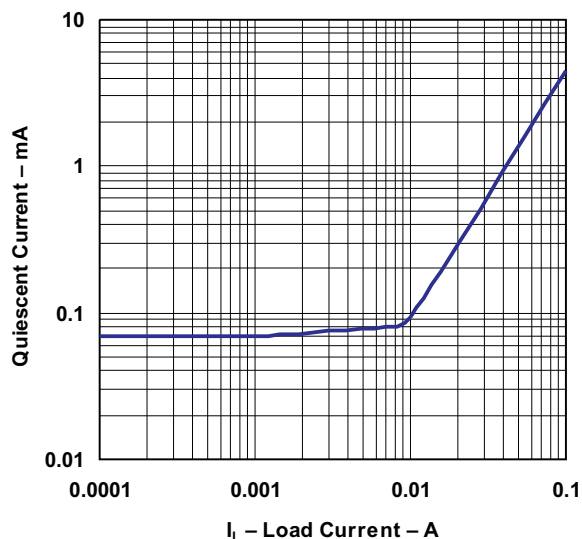
$V_{IN} = V_{OUT}$  (nominal) + 1 V,  $I_L = 100\ \mu\text{A}$ ,  $C_L = 1\ \mu\text{F}$  (5-V versions) or  $C_L = 2.2\ \mu\text{F}$  (3.3-V versions),  
8-pin version: FEEDBACK tied to  $V_{TAP}$ , OUTPUT tied to SENSE,  $V_{SHUTDOWN} \leq 0.7\ \text{V}$

PARAMETER	TEST CONDITIONS	$T_A$	MIN	TYP	MAX	UNIT
Thermal regulation <sup>(4)</sup>	$I_L = 100\ \mu\text{A}$	25°C		0.05	0.2	%/W
Output noise (RMS), 10 Hz to 100 kHz	$C_L = 1\ \mu\text{F}$ (5 V only)	25°C		430		$\mu\text{V}$
	$C_L = 200\ \mu\text{F}$			160		
	LP2951-50-Q1: $C_L = 3.3\ \mu\text{F}$ , $C_{Bypass} = 0.01\ \mu\text{F}$ between pins 1 and 7			100		
Reference voltage	$V_{OUT} = V_{REF}$ to $(V_{IN} - 1\ \text{V})$ , $V_{IN} = 2.3\ \text{V}$ to 30 V, $I_L = 100\ \mu\text{A}$ to 100 mA	–40°C to 125°C	1.200		1.272	V
Reference voltage temperature coefficient <sup>(1)</sup>		25°C		20		ppm/°C
<b>ERROR COMPARATOR</b>						
Output leakage current	$V_{OUT} = 30\ \text{V}$	25°C		0.01	1	$\mu\text{A}$
		–40°C to 125°C			2	
Output low voltage	$V_{IN} = V_{OUT(NOM)} - 0.5\ \text{V}$ , $I_{OL} = 400\ \mu\text{A}$	25°C		150	250	mV
		–40°C to 125°C			400	
Upper threshold voltage (ERROR output high) <sup>(5)</sup>		25°C	40	60		mV
		–40°C to 125°C	25			
Lower threshold voltage (ERROR output low) <sup>(5)</sup>		25°C		75	95	mV
		–40°C to 125°C			140	
Hysteresis <sup>(5)</sup>		25°C		15		mV
<b>SHUTDOWN INPUT</b>						
Input logic voltage	Low (regulator ON)	–40°C to 125°C			0.7	V
	High (regulator OFF)		2			
SHUTDOWN input current	$V_{TAP} = 2.4\ \text{V}$	25°C		30	50	$\mu\text{A}$
		–40°C to 125°C			100	
	$V_{TAP} = 30\ \text{V}$	25°C		450	600	
		–40°C to 125°C			750	
Regulator output current in shutdown	$V_{SHUTDOWN} \geq 2\ \text{V}$ , $V_{IN} \leq 30\ \text{V}$ , $V_{OUT} = 0$ , FEEDBACK tied to $V_{TAP}$	25°C		3	10	$\mu\text{A}$
		–40°C to 125°C			20	

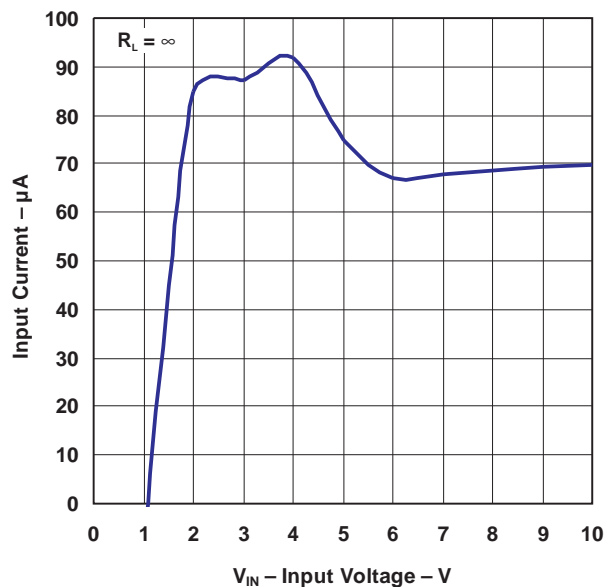
- (4) Thermal regulation is defined as the change in output voltage at a time (T) after a change in power dissipation is applied, excluding load or line regulation effects. Specifications are for a 50-mA load pulse at  $V_{IN} = 30\ \text{V}$ ,  $V_{OUT} = 5\ \text{V}$  (1.25-W pulse) for  $t = 10\ \text{ms}$ .
- (5) Comparator thresholds are expressed in terms of a voltage differential equal to the nominal reference voltage (measured at  $V_{IN} - V_{OUT} = 1\ \text{V}$ ) minus FEEDBACK terminal voltage. To express these thresholds in terms of output voltage change, multiply by the error amplifier gain  $= V_{OUT}/V_{REF} = (R1 + R2)/R2$ . For example, at a programmed output voltage of 5 V, the ERROR output is specified to go low when the output drops by  $95\ \text{mV} \times 5\ \text{V}/1.235\ \text{V} = 384\ \text{mV}$ . Thresholds remain constant as a percentage of  $V_{OUT}$  (as  $V_{OUT}$  is varied), with the low-output warning occurring at 6% below nominal (typ) and 7.7% (max).

## TYPICAL CHARACTERISTICS

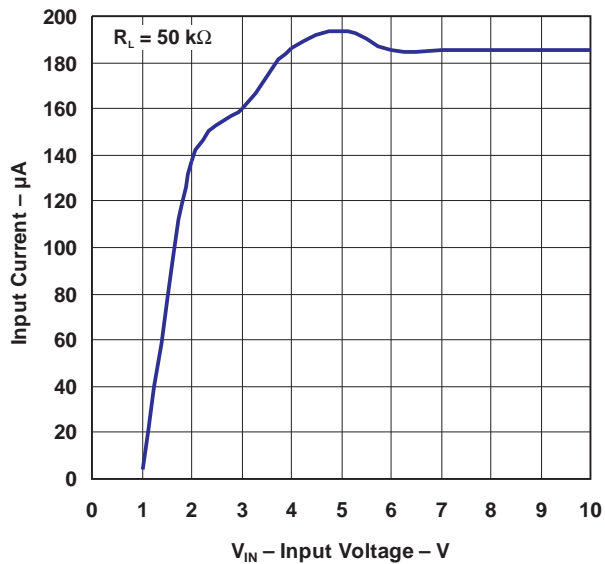
QUIESCENT CURRENT  
vs  
LOAD CURRENT



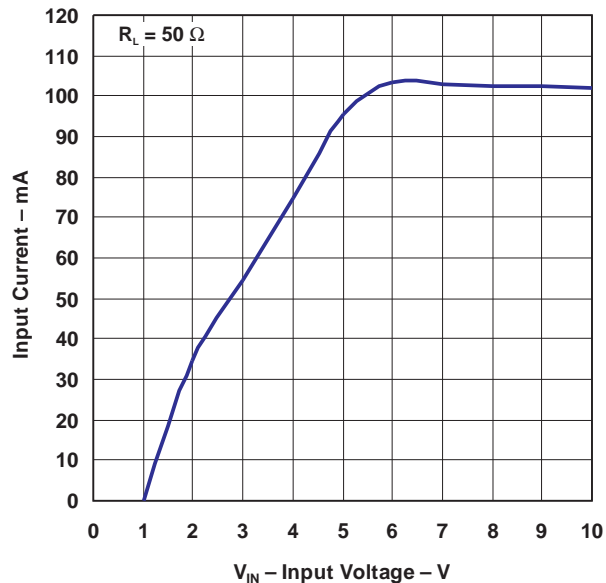
INPUT CURRENT  
vs  
INPUT VOLTAGE



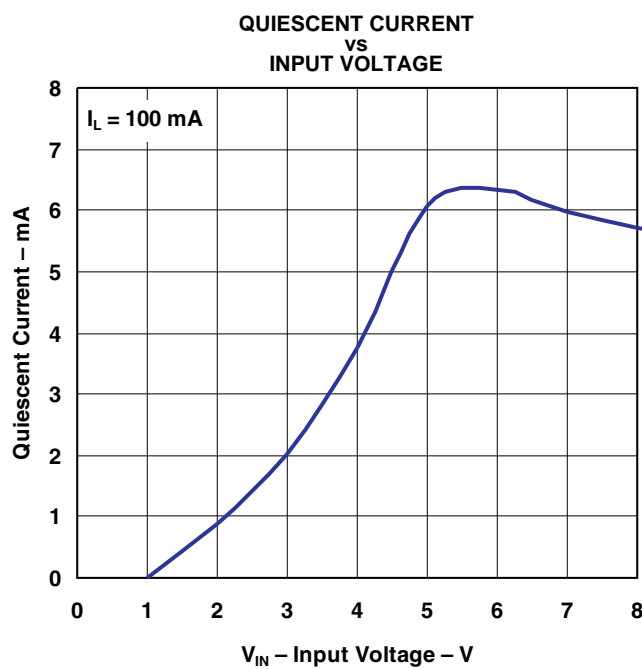
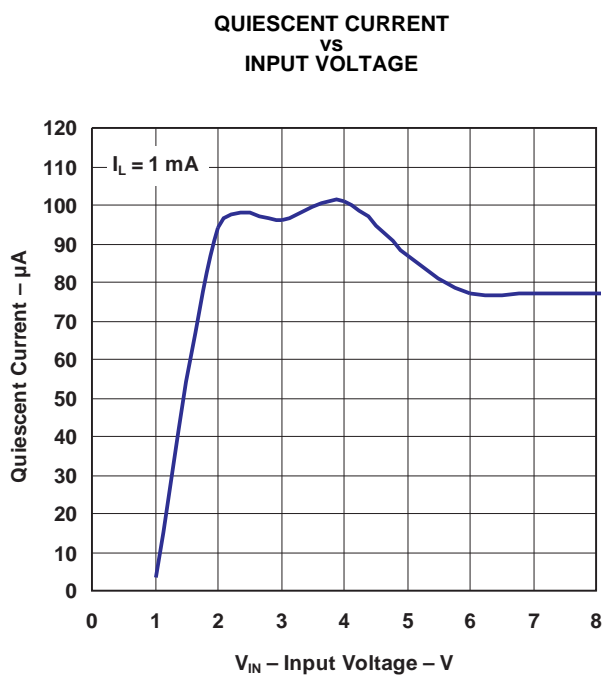
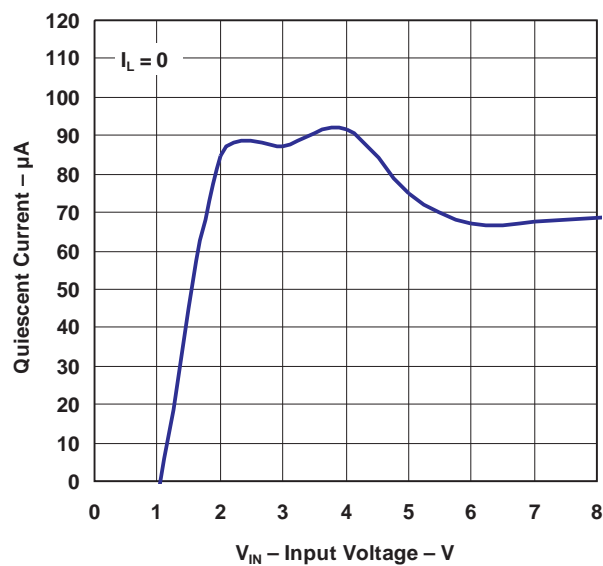
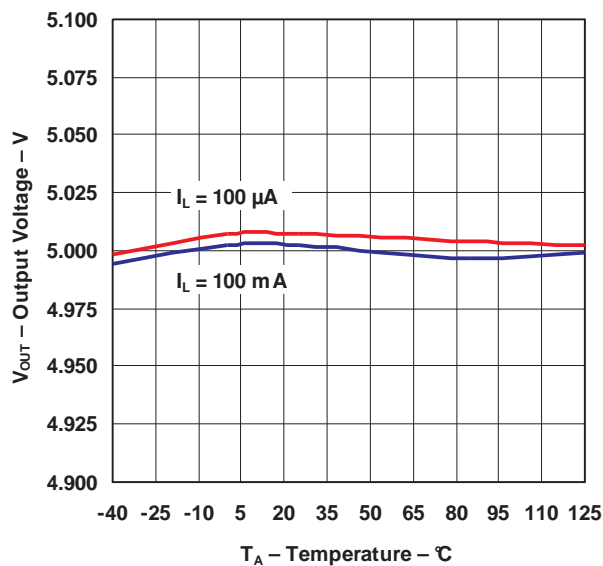
INPUT CURRENT  
vs  
INPUT VOLTAGE



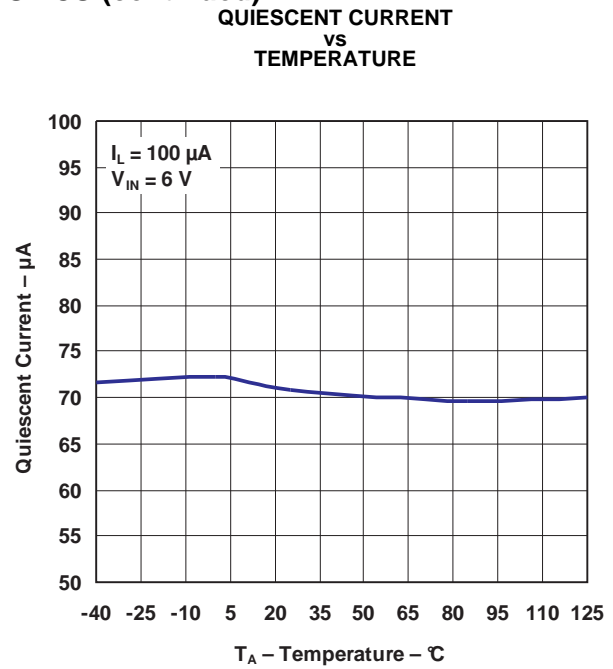
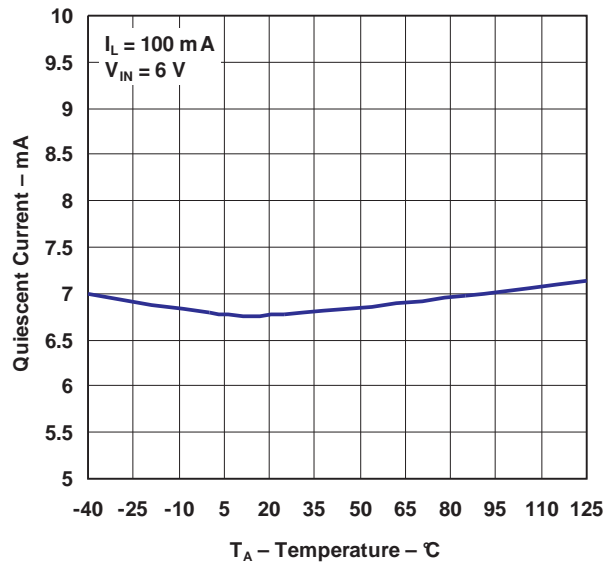
INPUT CURRENT  
vs  
INPUT VOLTAGE



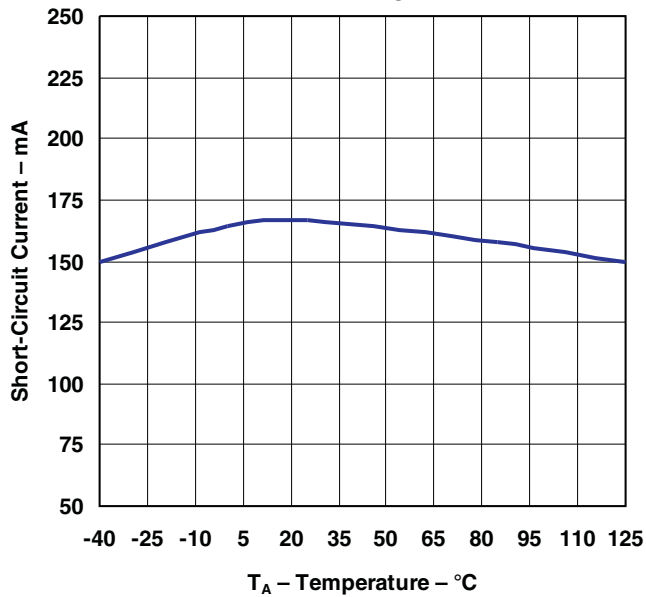
# TYPICAL CHARACTERISTICS (continued) OUTPUT VOLTAGE vs TEMPERATURE QUIESCENT CURRENT vs INPUT VOLTAGE



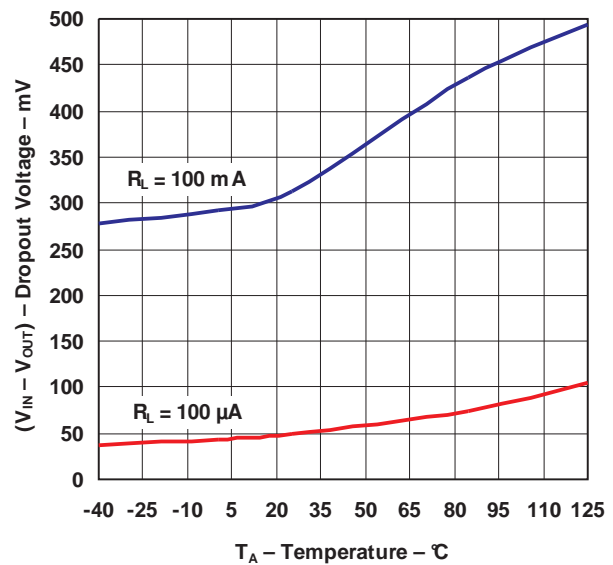
**TYPICAL CHARACTERISTICS (continued)**  
**QUIESCENT CURRENT**  
**VS**  
**TEMPERATURE**



**SHORT-CIRCUIT CURRENT**  
**VS**  
**TEMPERATURE**

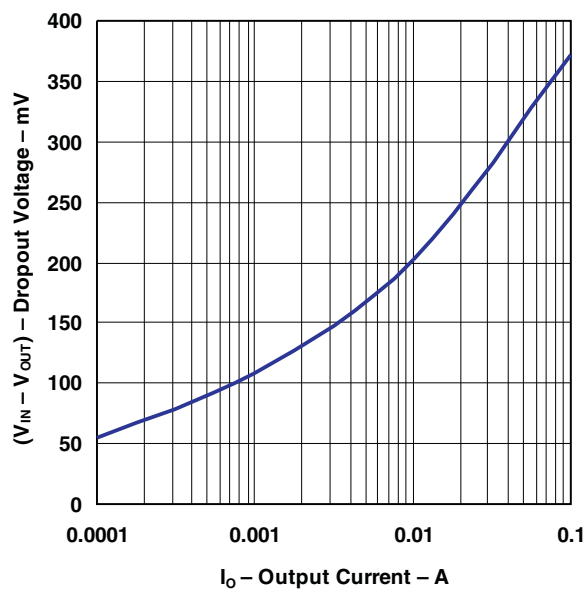


**DROPOUT VOLTAGE**  
**VS**  
**TEMPERATURE**

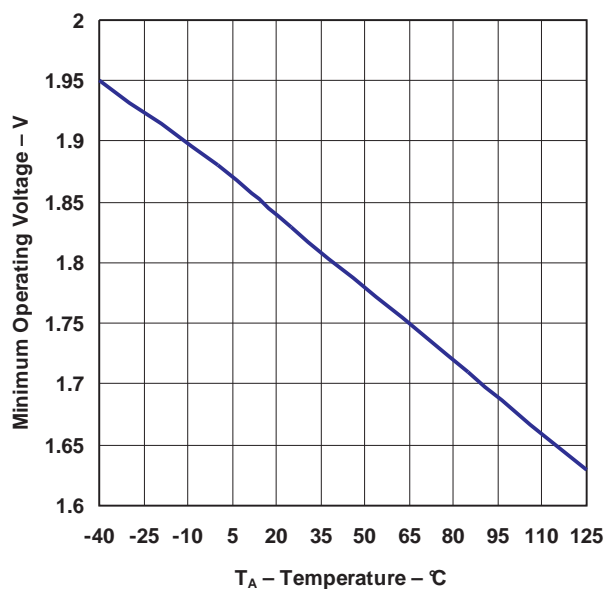


## TYPICAL CHARACTERISTICS (continued)

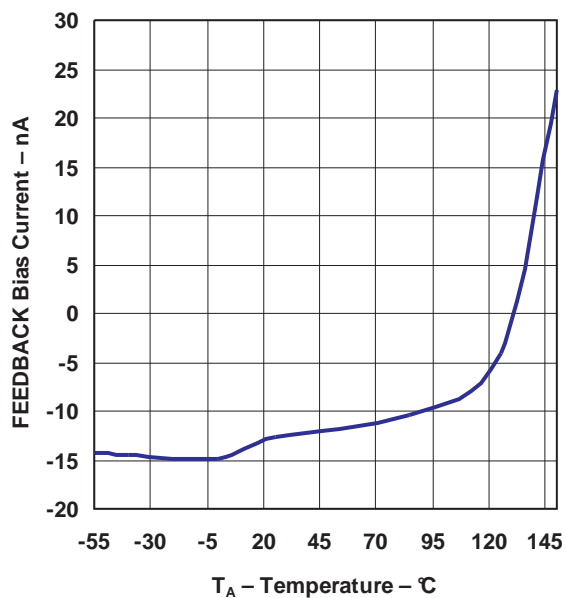
DROPOUT VOLTAGE  
vs  
OUTPUT CURRENT



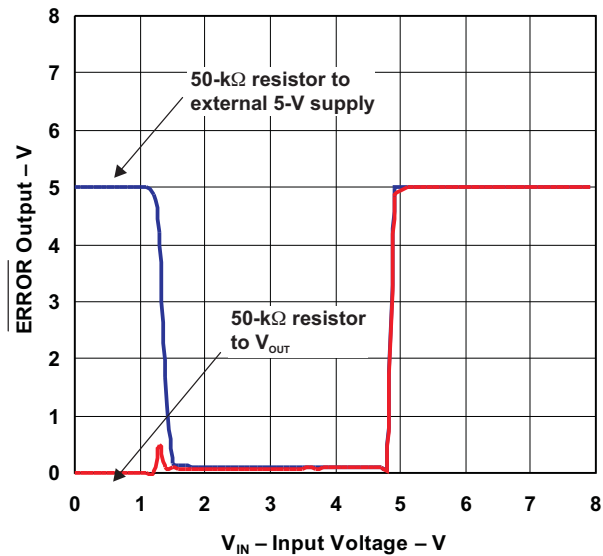
MINIMUM OPERATING VOLTAGE  
vs  
TEMPERATURE



FEEDBACK BIAS CURRENT  
vs  
TEMPERATURE

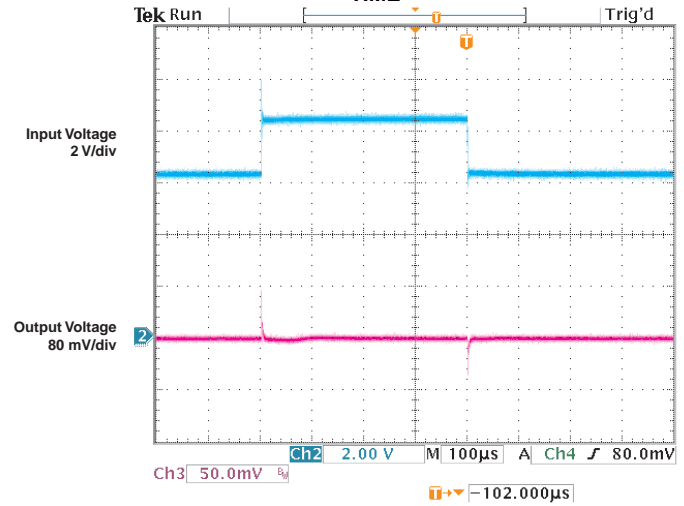
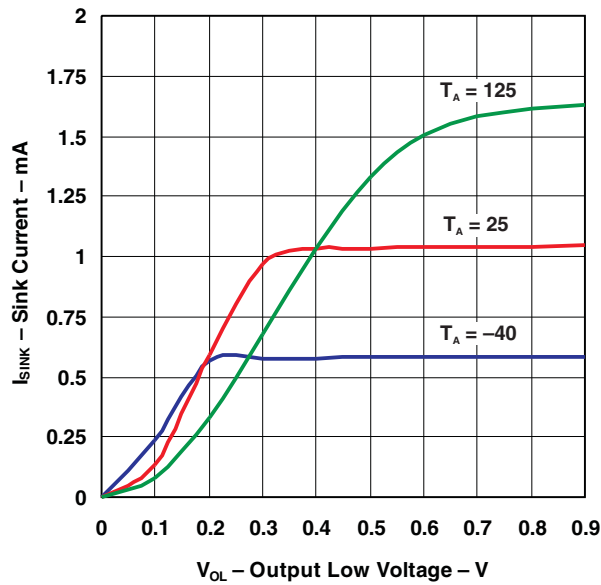


ERROR COMPARATOR OUTPUT  
vs  
INPUT VOLTAGE

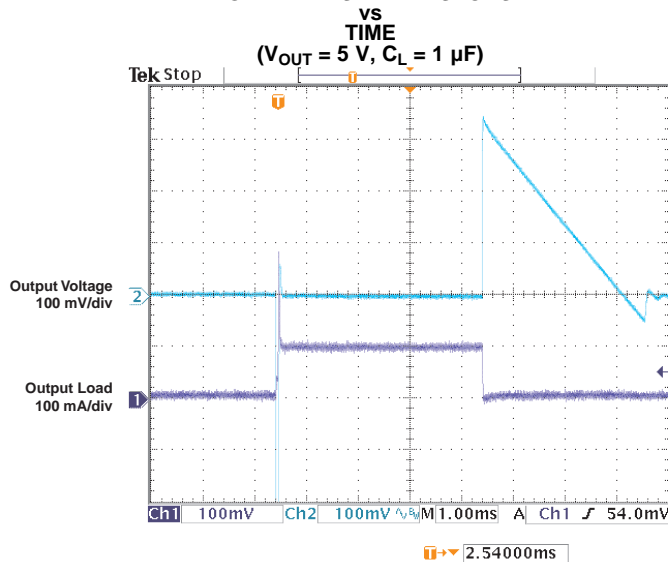




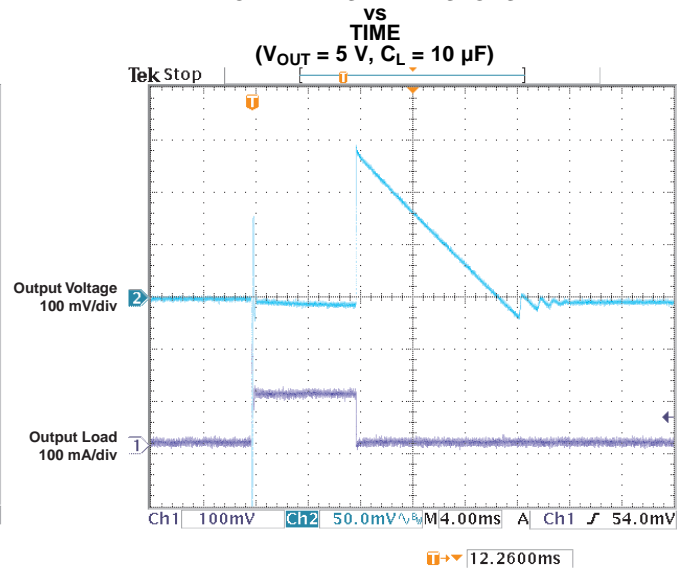
# **TYPICAL CHARACTERISTICS (continued)** **ERROR COMPARATOR SINK CURRENT** VS **OUTPUT LOW VOLTAGE** **LINE TRANSIENT RESPONSE** VS **TIME**



## **LOAD TRANSIENT RESPONSE**



## **LOAD TRANSIENT RESPONSE**

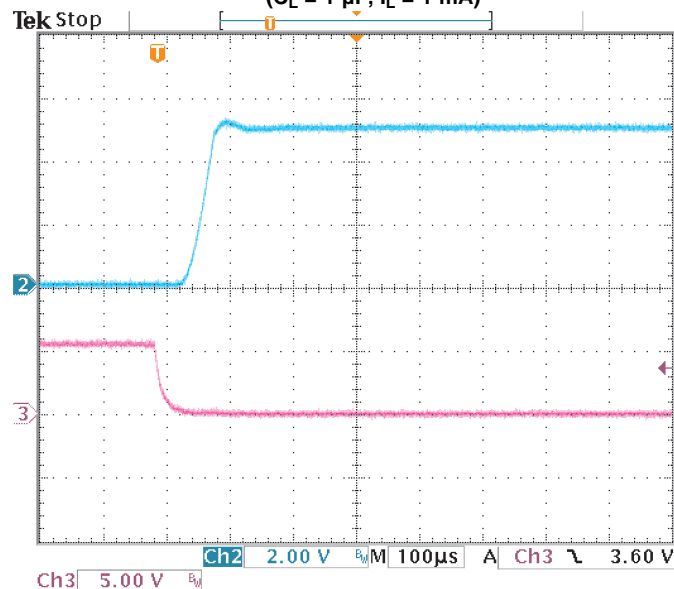


# TYPICAL CHARACTERISTICS (continued)

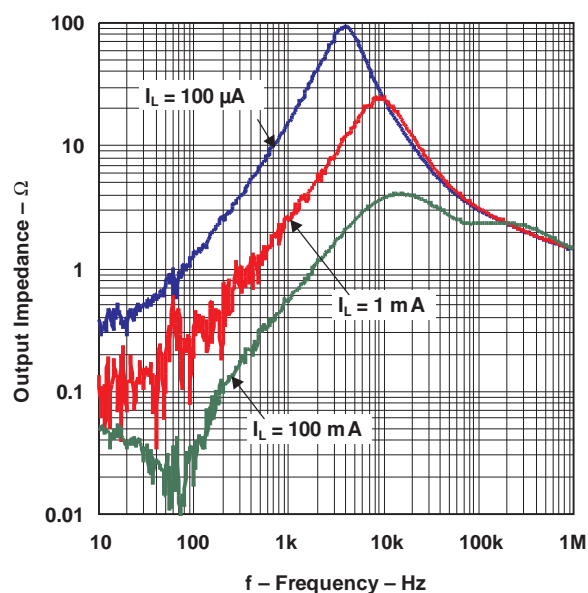
ENABLE TRANSIENT RESPONSE

VS  
TIME

( $C_L = 1 \mu\text{F}$ ,  $I_L = 1 \text{ mA}$ )



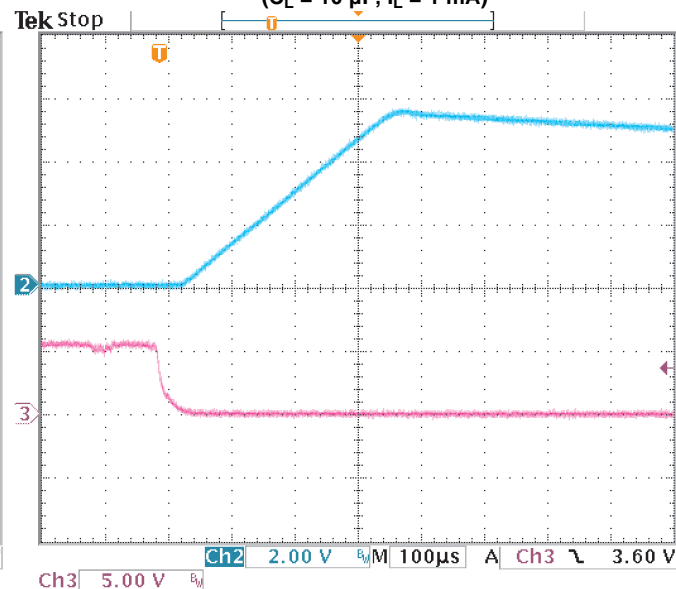
OUTPUT IMPEDANCE  
VS  
FREQUENCY



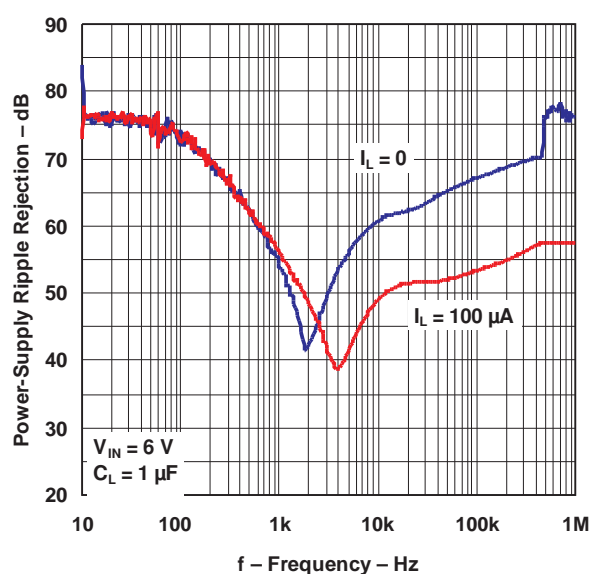
ENABLE TRANSIENT RESPONSE

VS  
TIME

( $C_L = 10 \mu\text{F}$ ,  $I_L = 1 \text{ mA}$ )

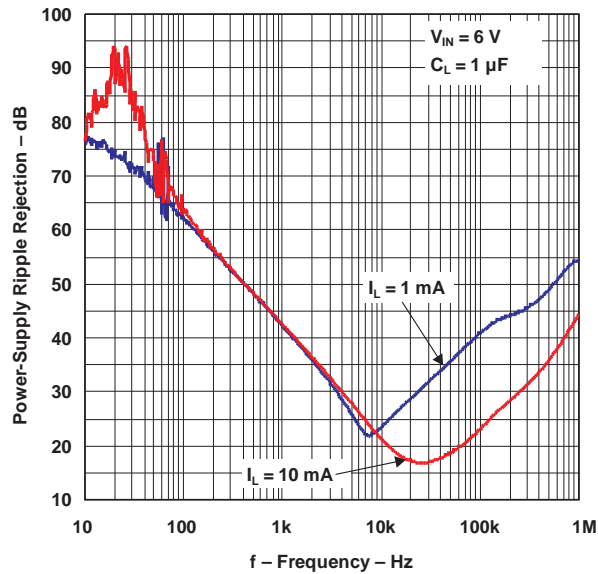


RIPPLE REJECTION  
VS  
FREQUENCY

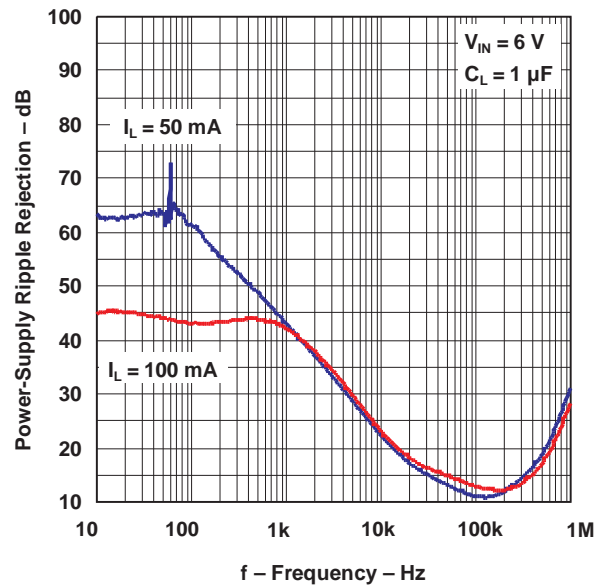


## TYPICAL CHARACTERISTICS (continued)

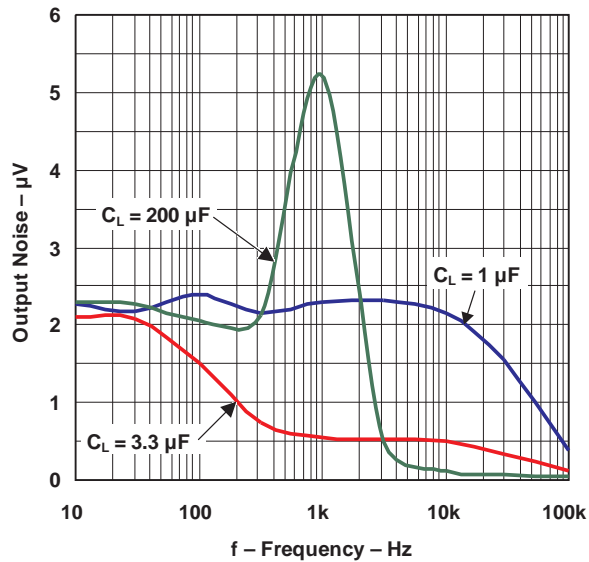
RIPPLE REJECTION  
VS  
FREQUENCY



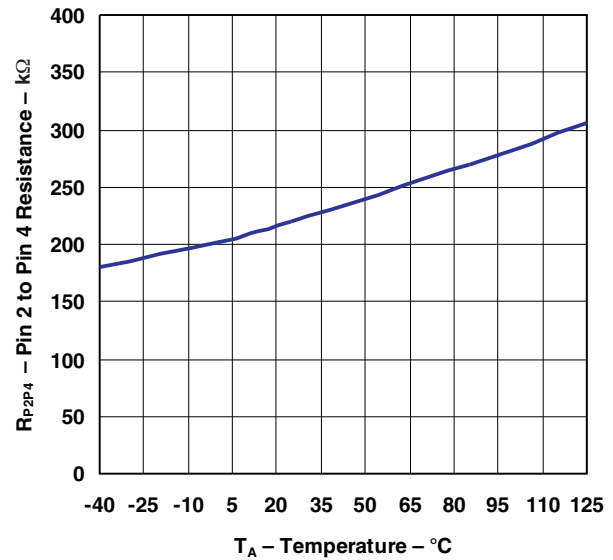
RIPPLE REJECTION  
VS  
FREQUENCY



OUTPUT NOISE  
VS  
FREQUENCY

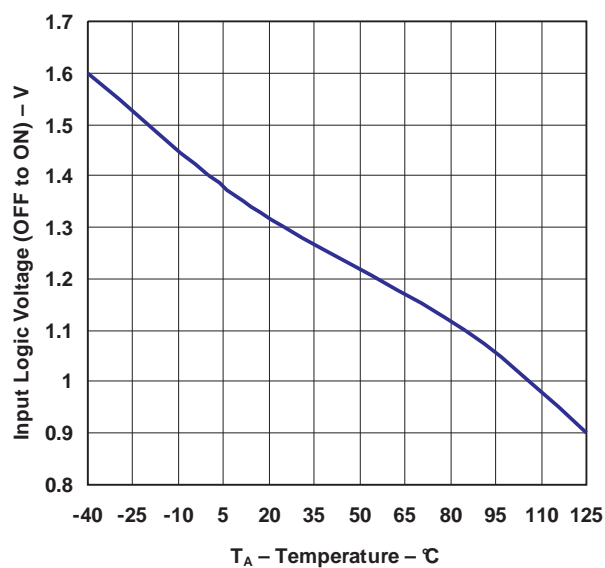


DIVIDER RESISTANCE  
VS  
TEMPERATURE

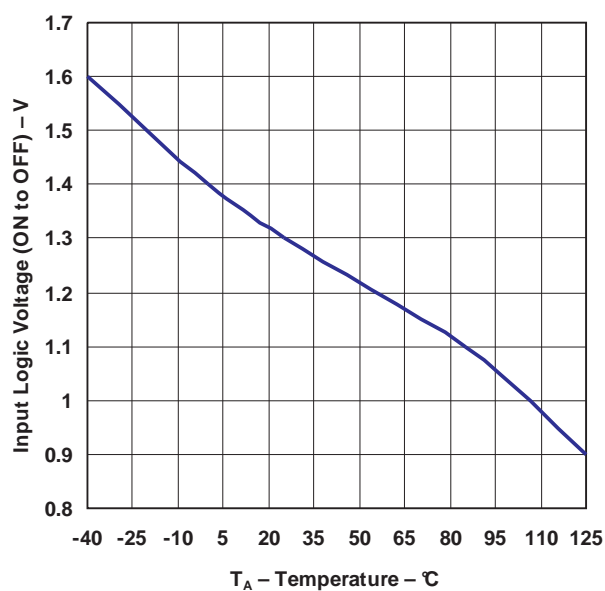


## TYPICAL CHARACTERISTICS (continued)

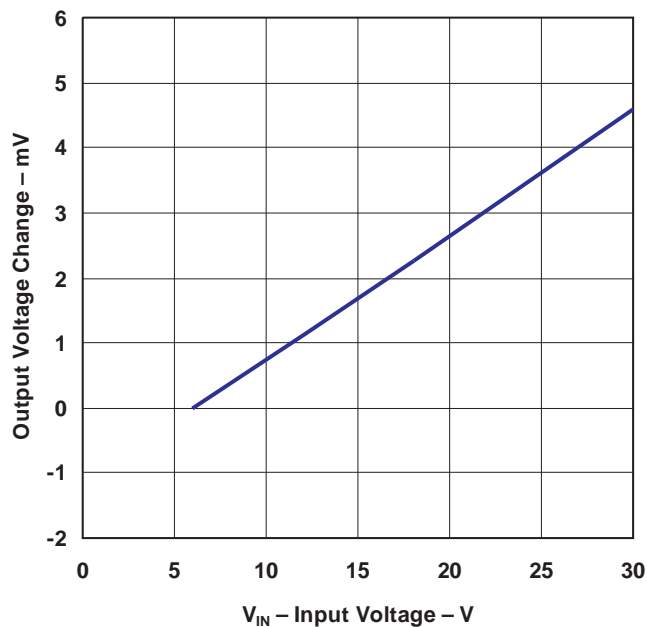
SHUTDOWN THRESHOLD VOLTAGE (OFF TO ON)  
vs  
TEMPERATURE



SHUTDOWN THRESHOLD VOLTAGE (ON TO OFF)  
vs  
TEMPERATURE



LINE REGULATION  
vs  
INPUT VOLTAGE



## APPLICATION INFORMATION

### Input Capacitor ( $C_{IN}$ )

A 1- $\mu$ F (tantalum, ceramic, or aluminum) electrolytic capacitor should be placed locally at the input of the LP2951-xx-Q1 if there is, or will be, significant impedance between the ac filter capacitor and the input; for example, if a battery is used as the input or if the ac filter capacitor is located more than 10 in away. There are no ESR requirements for this capacitor, and the capacitance can be increased without limit.

### Output Capacitor ( $C_{OUT}$ )

As with most PNP LDOs, stability conditions require the output capacitor to have a minimum capacitance and an ESR that falls within a certain range.

### Capacitance Value

For  $V_{OUT} \geq 5$  V, a minimum of 1  $\mu$ F is required. For lower  $V_{OUT}$ , the regulator's loop gain is running closer to unity gain and, thus, has lower phase margins. Consequently, a larger capacitance is needed for stability. For  $V_{OUT} = 3.3$  V, a minimum of 2.2  $\mu$ F is recommended. For worst case,  $V_{OUT} = 1.23$  V (using the ADJ version), a minimum of 3.3  $\mu$ F is recommended.  $C_{OUT}$  can be increased without limit and only improves the regulator stability and transient response. Regardless of its value, the output capacitor should have a resonant frequency less than 500 kHz.

The minimum capacitance values given above are for maximum load current of 100 mA. If the maximum expected load current is less than 100 mA, then lower values of  $C_{OUT}$  can be used. For instance, if  $I_{OUT} < 10$  mA, then only 0.33  $\mu$ F is required for  $C_{OUT}$ . For  $I_{OUT} < 1$  mA, 0.1  $\mu$ F is sufficient for stability requirements. Thus, for a worst-case condition of 100-mA load and  $V_{OUT} = V_{REF} = 1.235$  V (representing the highest load current and lowest loop gain), a minimum  $C_{OUT}$  of 3.3  $\mu$ F is recommended.

The LP2951-xx-Q1 is used with external resistors to set the output voltage, a minimum load current of 1  $\mu$ A is recommended through the resistor divider.

### ESR Range

The regulator control loop relies on the ESR of the output capacitor to provide a zero to add sufficient phase margin to ensure unconditional regulator stability; this requires the closed-loop gain to intersect the open-loop response in a region where the open-loop gain rolls off at 20 dB/decade. This ensures that the phase always is less than 180° (phase margin greater than 0°) at unity gain. Thus, a minimum-maximum range for the ESR must be observed.

The upper limit of this ESR range is established by the fact that too high an ESR could result in the zero occurring too soon, causing the gain to roll off too slowly, which, in turn allows a third pole to appear before unity gain and introduce enough phase shift to cause instability. This typically limits the max ESR to approximately 5  $\Omega$ .

Conversely, the lower limit of the ESR is tied to the fact that too low an ESR shifts the zero too far out (past unity gain) and, thus, allows the gain to roll off at 40 dB/decade at unity gain, with a resulting phase shift of greater than 180°. Typically, this limits the minimum ESR to approximately 20 m $\Omega$  to 30 m $\Omega$ .

For specific ESR requirements, see *Typical Characteristics*.

## Capacitor Types

Most tantalum or aluminum electrolytics are suitable for use at the input. Film-type capacitors also work, but at higher cost. When operating at low temperature, care should be taken with aluminum electrolytics, as their electrolytes often freeze at  $-30^{\circ}\text{C}$ . For this reason, solid tantalum capacitors should be used at temperatures below  $-25^{\circ}\text{C}$ .

Ceramic capacitors can be used, but due to their low ESR (as low as  $5\text{ m}\Omega$  to  $10\text{ m}\Omega$ ), they may not meet the minimum ESR requirement previously discussed. If a ceramic capacitor is used, a series resistor between  $0.1\text{ }\Omega$  to  $2\text{ }\Omega$  must be added to meet the minimum ESR requirement. In addition, ceramic capacitors have one glaring disadvantage that must be taken into account — a poor temperature coefficient, where the capacitance can vary significantly with temperature. For instance, a large-value ceramic capacitor ( $\geq 2.2\text{ }\mu\text{F}$ ) can lose more than half of its capacitance as temperature rises from  $25^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ . Thus, a  $2.2\text{-}\mu\text{F}$  capacitor at  $25^{\circ}\text{C}$  drops well below the minimum  $C_{\text{OUT}}$  required for stability as ambient temperature rises. For this reason, select an output capacitor that maintains the minimum  $2.2\text{ }\mu\text{F}$  required for stability for the entire operating temperature range.

## $C_{\text{BYPASS}}$ : Noise and Stability Improvement

In the LP2951-xx-Q1, an external FEEDBACK pin directly connected to the error amplifier noninverting input can allow stray capacitance to cause instability by shunting the error amplifier feedback to GND, especially at high frequencies. This is worsened if high-value external resistors are used to set the output voltage, because a high resistance allows the stray capacitance to play a more significant role; i.e., a larger RC time delay is introduced between the output of the error amplifier and its FEEDBACK input, leading to more phase shift and lower phase margin. A solution is to add a  $100\text{-pF}$  bypass capacitor ( $C_{\text{BYPASS}}$ ) between OUTPUT and FEEDBACK; because  $C_{\text{BYPASS}}$  is in parallel with  $R1$ , it lowers the impedance seen at FEEDBACK at high frequencies, in effect offsetting the effect of the parasitic capacitance by providing more feedback at higher frequencies. More feedback forces the error amplifier to work at a lower loop gain, so  $C_{\text{OUT}}$  should be increased to a minimum of  $3.3\text{ }\mu\text{F}$  to improve the regulator's phase margin.

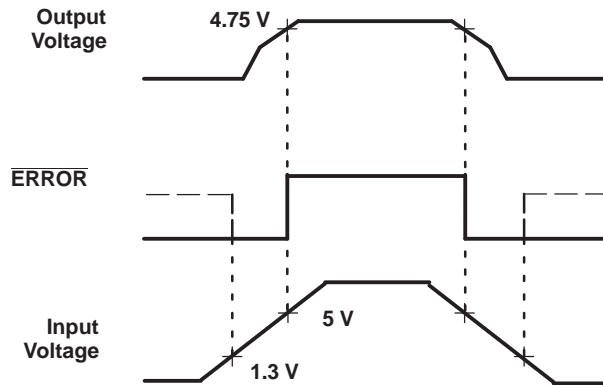
$C_{\text{BYPASS}}$  can be also used to reduce output noise in the LP2951-xx-Q1. This bypass capacitor reduces the closed loop gain of the error amplifier at the high frequency, so noise no longer scales with the output voltage. This improvement is more noticeable with higher output voltages, because loop gain reduction is greatest. A suitable  $C_{\text{BYPASS}}$  is calculated as shown in [Equation 1](#):

$$f_{(\text{CBYPASS})} \approx 200\text{ Hz} \rightarrow C_{\text{BYPASS}} = \frac{1}{2\pi \times R1 \times 200\text{ Hz}} \quad (1)$$

## ERROR Function

The LP2951-xx-Q1 has a low-voltage detection comparator that outputs a logic low when the output voltage drops by  $\pm 6\%$  from its nominal value, and outputs a logic high when  $V_{\text{OUT}}$  has reached  $\pm 95\%$  of its nominal value. This 95% of nominal figure is obtained by dividing the built-in offset of  $\pm 60\text{ mV}$  by the  $1.235\text{-V}$  bandgap reference, and remains independent of the programmed output voltage. For example, the trip-point threshold (ERROR output goes high) typically is  $4.75\text{ V}$  for a  $5\text{-V}$  output and  $11.4\text{ V}$  for a  $12\text{-V}$  output. Typically, there is a hysteresis of  $15\text{ mV}$  between the thresholds for high and low ERROR output.

A timing diagram is shown in [Figure 1](#) for  $\overline{\text{ERROR}}$  vs  $V_{\text{OUT}}$  ( $5\text{ V}$ ), as  $V_{\text{IN}}$  is ramped up and down.  $\overline{\text{ERROR}}$  becomes valid (low) when  $V_{\text{IN}} \neq 1.3\text{ V}$ . When  $V_{\text{IN}} \neq 5\text{ V}$ ,  $V_{\text{OUT}} = 4.75\text{ V}$ , causing  $\overline{\text{ERROR}}$  to go high. Because the dropout voltage is load dependent, the output trip-point threshold is reached at different values of  $V_{\text{IN}}$ , depending on the load current. For instance, at higher load current,  $\overline{\text{ERROR}}$  goes high at a slightly higher value of  $V_{\text{IN}}$ , and vice versa for lower load current. The output-voltage trip point remains at  $\pm 4.75\text{ V}$ , regardless of the load. Note that when  $V_{\text{IN}} \leq 1.3\text{ V}$ , the ERROR comparator output is turned off and pulled high to its pullup voltage. If  $V_{\text{OUT}}$  is used as the pullup voltage, rather than an external  $5\text{-V}$  source, ERROR typically is  $\pm 1.2\text{ V}$ . In this condition, an equal resistor divider ( $10\text{ k}\Omega$  is suitable) can be tied to  $\overline{\text{ERROR}}$  to divide down the voltage to a valid logic low during any fault condition, while still enabling a logic high during normal operation.



**Figure 1.  $\overline{\text{ERROR}}$  Output Timing**

Because the  $\overline{\text{ERROR}}$  comparator has an open-collector output, an external pullup resistor is required to pull the output up to  $V_{\text{OUT}}$  or another supply voltage (up to 30 V). The output of the comparator is rated to sink up to 400  $\mu\text{A}$ . A suitable range of values for the pullup resistor is from 100 k $\Omega$  to 1 M $\Omega$ . If ERROR is not used, it can be left open.

### Programming Output Voltage

A unique feature of the LP2951-xx-Q1 is its ability to output either a fixed voltage or an adjustable voltage, depending on the external pin connections. To output the internally programmed fixed voltage, tie the SENSE pin to the OUTPUT pin and the FEEDBACK pin to the  $V_{\text{TAP}}$  pin. Alternatively, a user-programmable voltage ranging from the internal 1.235-V reference to a 30-V max can be set by using an external resistor divider pair. The resistor divider is tied to  $V_{\text{OUT}}$ , and the divided-down voltage is tied directly to FEEDBACK for comparison against the internal 1.235-V reference. To satisfy the steady-state condition in which its two inputs are equal, the error amplifier drives the output to equal [Equation 2](#):

$$V_{\text{OUT}} = V_{\text{REF}} \times \left( 1 + \frac{R1}{R2} \right) - I_{\text{FB}}R_1 \quad (2)$$

Where:

$V_{\text{REF}} = 1.235 \text{ V}$  applied across R2

$I_{\text{FB}} = \text{FEEDBACK bias current, typically } 20 \text{ nA}$

A minimum regulator output current of 1  $\mu\text{A}$  must be maintained. Thus, in an application where a no-load condition is expected (for example, CMOS circuits in standby), this 1- $\mu\text{A}$  minimum current must be provided by the resistor pair, effectively imposing a maximum value of  $R2 = 1.2 \text{ M}\Omega$  ( $1.235 \text{ V}/1.2 \text{ M}\Omega \approx 1 \mu\text{A}$ ).

$I_{\text{FB}} = 20 \text{ nA}$  introduces an error of  $\approx 0.02\%$  in  $V_{\text{OUT}}$ . This can be offset by trimming R1. Alternatively, increasing the divider current makes  $I_{\text{FB}}$  less significant, thus, reducing its error contribution. For instance, using  $R2 = 100 \text{ k}\Omega$  reduces the error contribution of  $I_{\text{FB}}$  to 0.17% by increasing the divider current to  $\approx 12 \mu\text{A}$ . This increase in the divider current still is small compared to the 600- $\mu\text{A}$  typical quiescent current of the LP2951-xx-Q1 under no load.

## REVISION HISTORY

Changes from Original (June, 2011) to Revision A	Page
<ul style="list-style-type: none"> <li>Removed continuous from input voltage range parameter description; changed max values for <math>V_{IN}</math> and <math>V_{SHDN}</math> from 30 to 35. ....</li> </ul>	2
Changes from Revision A (July 2012) to Revision B	Page
<ul style="list-style-type: none"> <li>Changed LP2951-33QDRGRQ1 From: Preview To: Active .....</li> </ul>	1
Changes from Revision B (December 2012) to Revision C	Page
<ul style="list-style-type: none"> <li>Deleted P/N LP2951-Q1 from page header .....</li> </ul>	1
<ul style="list-style-type: none"> <li>Deleted ORDERING INFORMATION table .....</li> </ul>	1
Changes from Revision B (February 2013) to Revision D	Page
<ul style="list-style-type: none"> <li>Deleted unreleased devices .....</li> </ul>	1
<ul style="list-style-type: none"> <li>Added the THERMAL INFORMATION table .....</li> </ul>	3



## PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish	MSL Peak Temp (3)	Op Temp (°C)	Top-Side Markings (4)	Samples
LP2951-33QDRGRQ1	ACTIVE	SON	DRG	8	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	RACQ	<a href="#">Samples</a>
LP2951-50QDRGRQ1	ACTIVE	SON	DRG	8	3000	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 125	ZUFQ	<a href="#">Samples</a>

(1) The marketing status values are defined as follows:

**ACTIVE:** Product device recommended for new designs.

**LIFEBUY:** TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

**NRND:** Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

**PREVIEW:** Device has been announced but is not in production. Samples may or may not be available.

**OBsolete:** TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

**TBD:** The Pb-Free/Green conversion plan has not been defined.

**Pb-Free (RoHS):** TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

**Pb-Free (RoHS Exempt):** This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

**Green (RoHS & no Sb/Br):** TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. -- The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) Multiple Top-Side Markings will be inside parentheses. Only one Top-Side Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Top-Side Marking for that device.

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**OTHER QUALIFIED VERSIONS OF LP2951-33-Q1, LP2951-50-Q1, LP2951-Q1 :**

- 
- Catalog: [LP2951-33](#), [LP2951-50](#), [LP2951](#)

NOTE: Qualified Version Definitions:

- Catalog - TI's standard catalog product

**TAPE AND REEL INFORMATION**


\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LP2951-33QDRGRQ1	SON	DRG	8	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
LP2951-50QDRGRQ1	SON	DRG	8	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2

## TAPE AND REEL BOX DIMENSIONS

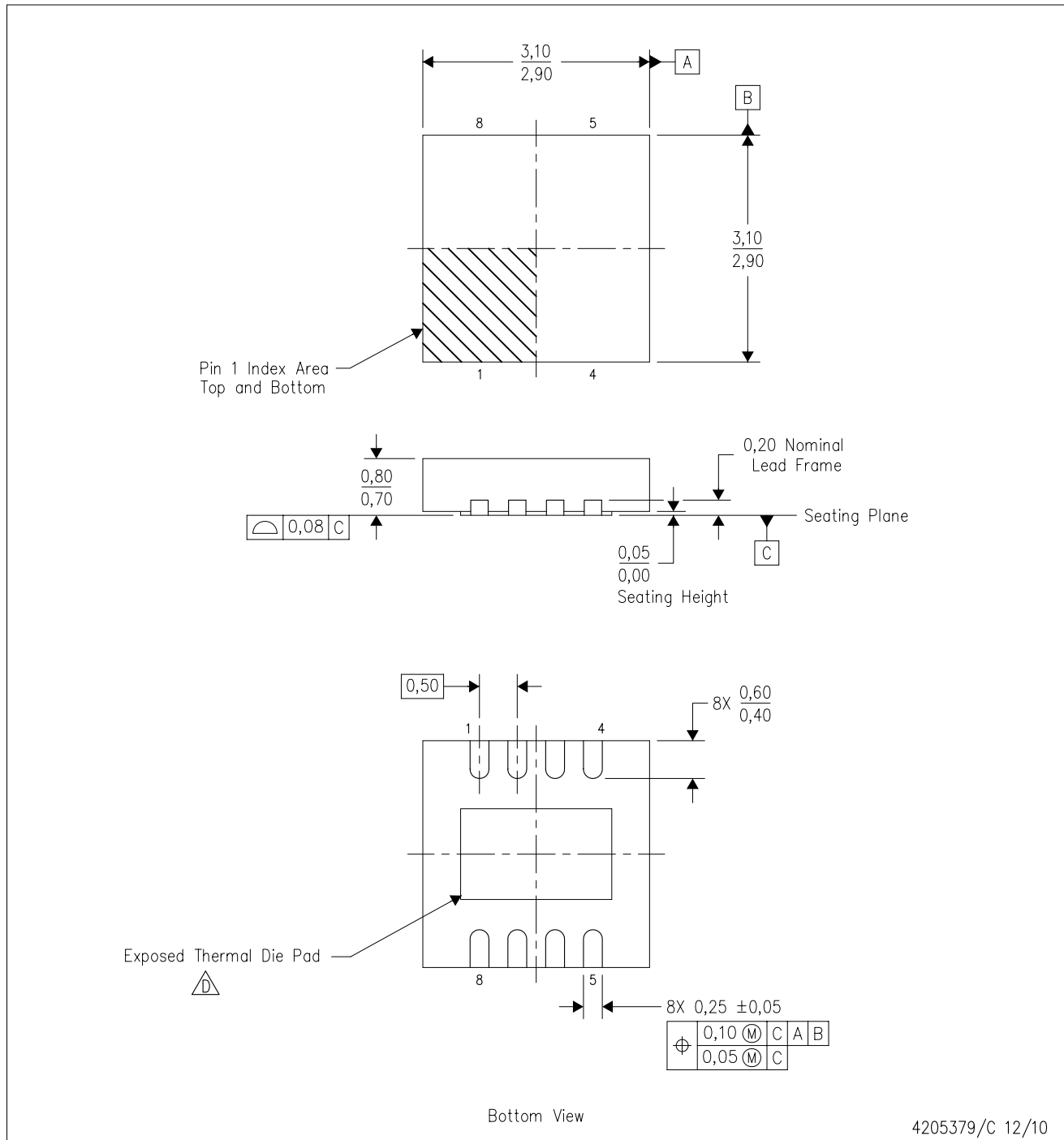



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LP2951-33QDRGRQ1	SON	DRG	8	3000	367.0	367.0	35.0
LP2951-50QDRGRQ1	SON	DRG	8	3000	367.0	367.0	35.0

DRG (S-PWSON-N8)

PLASTIC SMALL OUTLINE NO-LEAD



- NOTES:
- A. All linear dimensions are in millimeters. Dimensioning and tolerancing per ASME Y14.5M-1994.
  - B. This drawing is subject to change without notice.
  - C. SON (Small Outline No-Lead) package configuration.
  -  The package thermal pad must be soldered to the board for thermal and mechanical performance. See the Product Data Sheet for details regarding the exposed thermal pad dimensions.
  - E. JEDEC MO-229 package registration pending.

DRG (S-PWSON-N8)

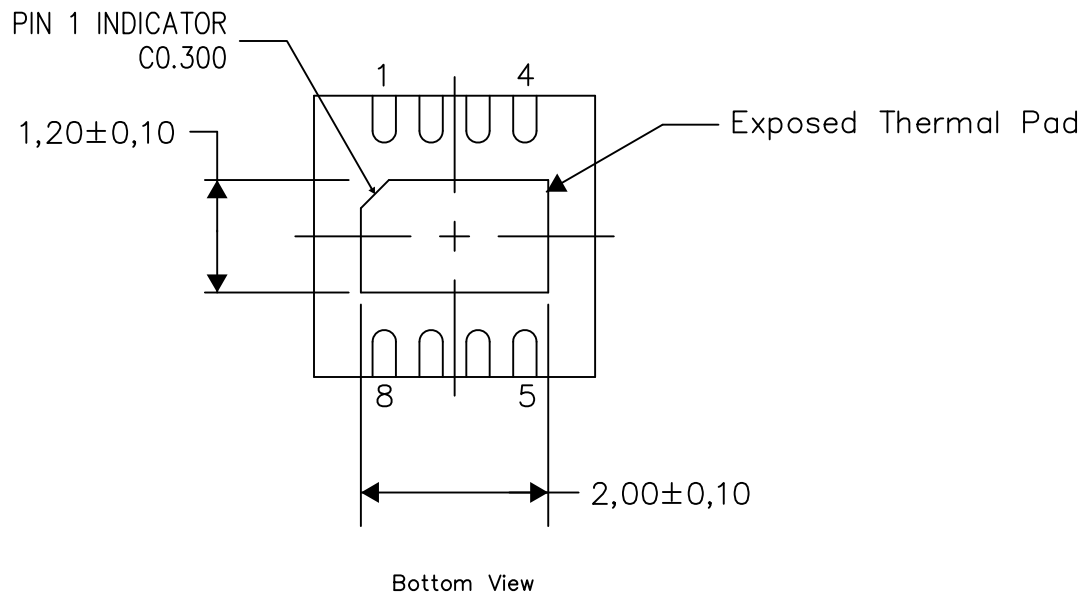
PLASTIC SMALL OUTLINE NO-LEAD

## THERMAL INFORMATION

This package incorporates an exposed thermal pad that is designed to be attached directly to an external heatsink. The thermal pad must be soldered directly to the printed circuit board (PCB). After soldering, the PCB can be used as a heatsink. In addition, through the use of thermal vias, the thermal pad can be attached directly to the appropriate copper plane shown in the electrical schematic for the device, or alternatively, can be attached to a special heatsink structure designed into the PCB. This design optimizes the heat transfer from the integrated circuit (IC).

For information on the Quad Flatpack No-Lead (QFN) package and its advantages, refer to Application Report, QFN/SON PCB Attachment, Texas Instruments Literature No. SLUA271. This document is available at [www.ti.com](http://www.ti.com).

The exposed thermal pad dimensions for this package are shown in the following illustration.



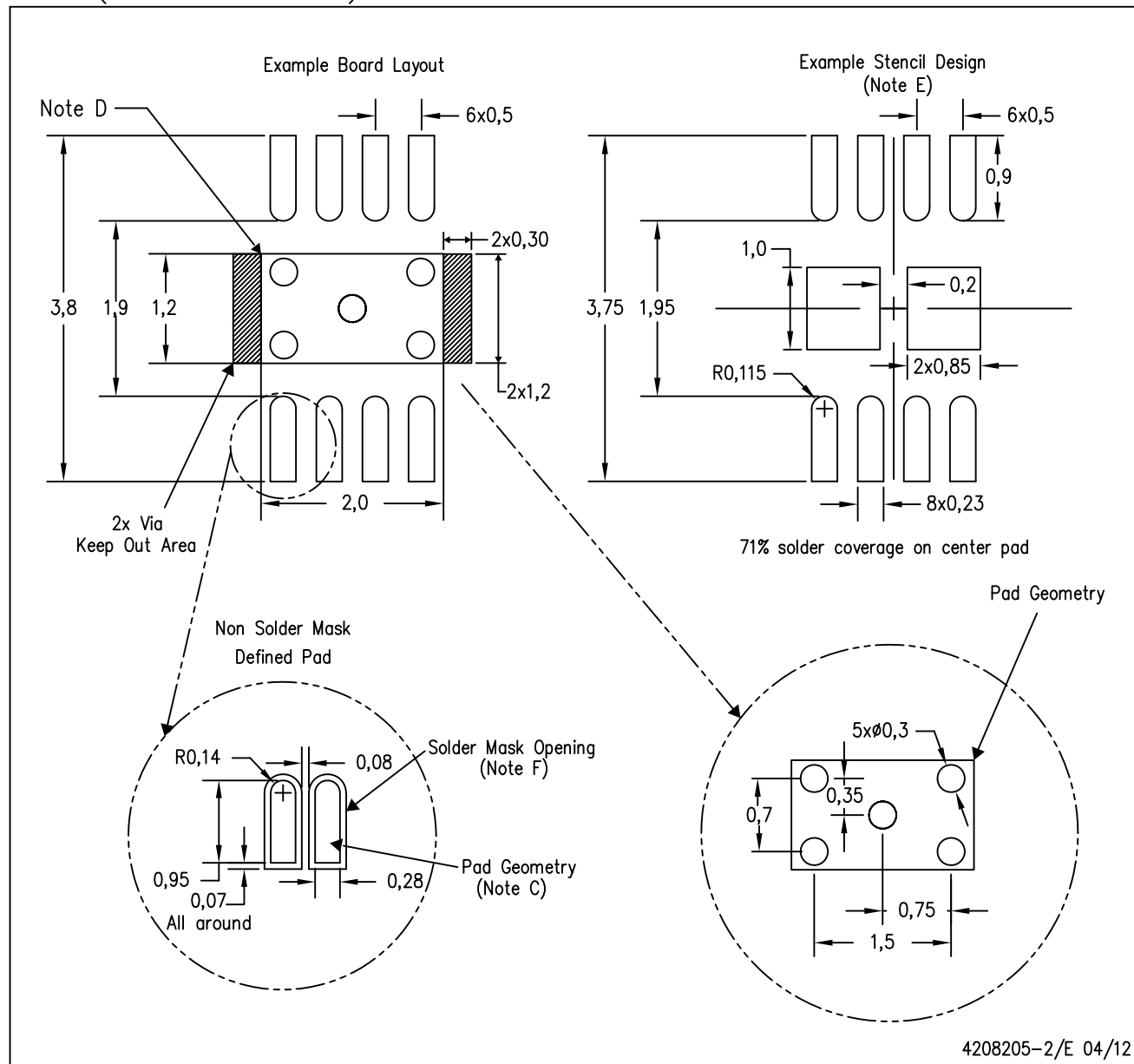
Exposed Thermal Pad Dimensions

4206881-2/G 04/12

NOTE: All linear dimensions are in millimeters

DRG (S-PWSON-N8)

PLASTIC SMALL OUTLINE NO-LEAD



- NOTES:
- All linear dimensions are in millimeters.
  - This drawing is subject to change without notice.
  - Publication IPC-SM-782 is recommended for alternate designs.
  - This package is designed to be soldered to a thermal pad on the board. Refer to Application Note, Quad Flat-Pack Packages, Texas Instruments Literature No. SLUA271, and also the Product Data Sheets for specific thermal information, via requirements, and recommended board layout. These documents are available at [www.ti.com](http://www.ti.com) <<http://www.ti.com>>.
  - Laser cutting apertures with trapezoidal walls and also rounding corners will offer better paste release. Customers should contact their board assembly site for stencil design recommendations. Refer to IPC 7525 for stencil design considerations.
  - Customers should contact their board fabrication site for minimum solder mask web tolerances between signal pads.

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